ACT4065

Rev 3, 05-Jan-12

High Input 2A Step Down Converter

FEATURES

- 2A Output Current
- Up to 95% Efficiency
- Up to 28V Input Range
- 8μA Shutdown Supply Current
- 200kHz Switching Frequency
- Adjustable Output Voltage
- Cycle-by-Cycle Current Limit Protection
- Thermal Shutdown Protection
- Frequency Foldback at Short Circuit
- Stability with Wide Range of Capacitors, Including Low ESR Ceramic Capacitors
- SOP-8 Package

APPLICATIONS

- TFT LCD Monitors
- Portable DVDs
- Car-Powered or Battery-Powered Equipments
- Set-Top Boxes
- Telecom Power Supplies
- DSL and Cable Modems and Routers
- Termination Supplies

GENERAL DESCRIPTION

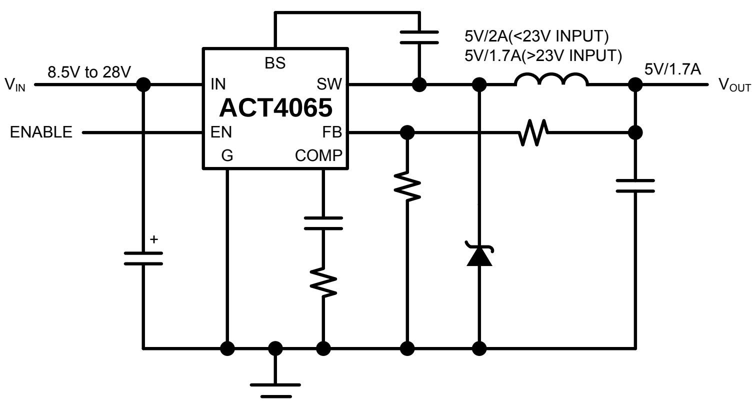
The ACT4065 is a current-mode step-down DC/DC converter that generates up to 2A output current at 200kHz switching frequency. The device utilizes Active-Semi's proprietary ISOBCD30 process for operation with input voltage up to 28V.

Consuming only 8μA in shutdown mode, the ACT4065 is highly efficient with peak efficiency at 95% when in operation. Protection features include cycle-by-cycle current limit, thermal shutdown, and frequency foldback at short circuit.

The ACT4065 is available in SOP-8 package and requires very few external devices for operation.

Note: ACT4065 is replaced by ACT4065A.

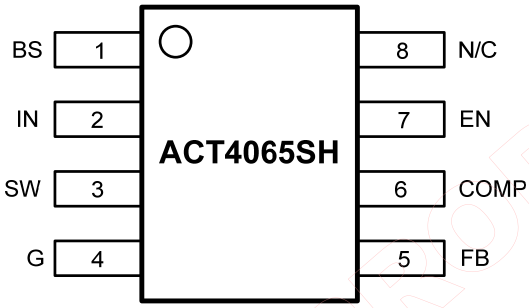
TYPICAL APPLICATION CIRCUIT



ORDERING INFORMATION

PART NUMBER	TEMPERATURE RANGE	PACKAGE	PINS	PACKING
ACT4065SH	-40°C to 85°C	SOP-8	8	TUBE
ACT4065SH-T	-40°C to 85°C	SOP-8	8	TAPE & REEL

PIN CONFIGURATION



SOP-8

PIN DESCRIPTION

PIN NUMBER	PIN NAME	PIN DESCRIPTION
1	BS	Bootstrap. This pin acts as the positive rail for the high-side switch's gate driver. Connect a 10nF between this pin and SW.
2	IN	Input Supply. Bypass this pin to G with a low ESR capacitor. See *Input Capacitor* in *Application Information* section.
3	SW	Switch Output. Connect this pin to the switching end of the inductor.
4	G	Ground.
5	FB	Feedback Input. The voltage at this pin is regulated to 1.293V. Connect to the resistor divider between output and ground to set output voltage.
6	COMP	Compensation Pin. See *Compensation Techniques* in *Application Information* section.
7	EN	Enable Input. When higher than 1.3V, this pin turns the IC on. When lower than 0.7V, this pin turn the IC off. Output voltage is discharged when the IC is off. This pin has a small internal pull-up current to a high level voltage when pin is not connected. Do not allow EN pin to exceed 6V.
8	N/C	Not Connected.

ABSOLUTE MAXIMUM RATINGS①

PARAMETER	VALUE	UNIT
IN Supply Voltage	-0.3 to 30	V
SW Voltage	-1 to V_{IN} + 1	V
BS Voltage	V_{SW} - 0.3 to V_{SW} + 8	V
EN, FB, COMP Voltage	-0.3 to 6	V
Continuous SW Current	Internally limited	A
Maximum Power Dissipation	0.76	W
Junction to Ambient Thermal Resistance (θ_{JA})	105	°C/W
Operating Junction Temperature	-40 to 150	°C
Storage Temperature	-55 to 150	°C
Lead Temperature (Soldering, 10 sec)	300	°C

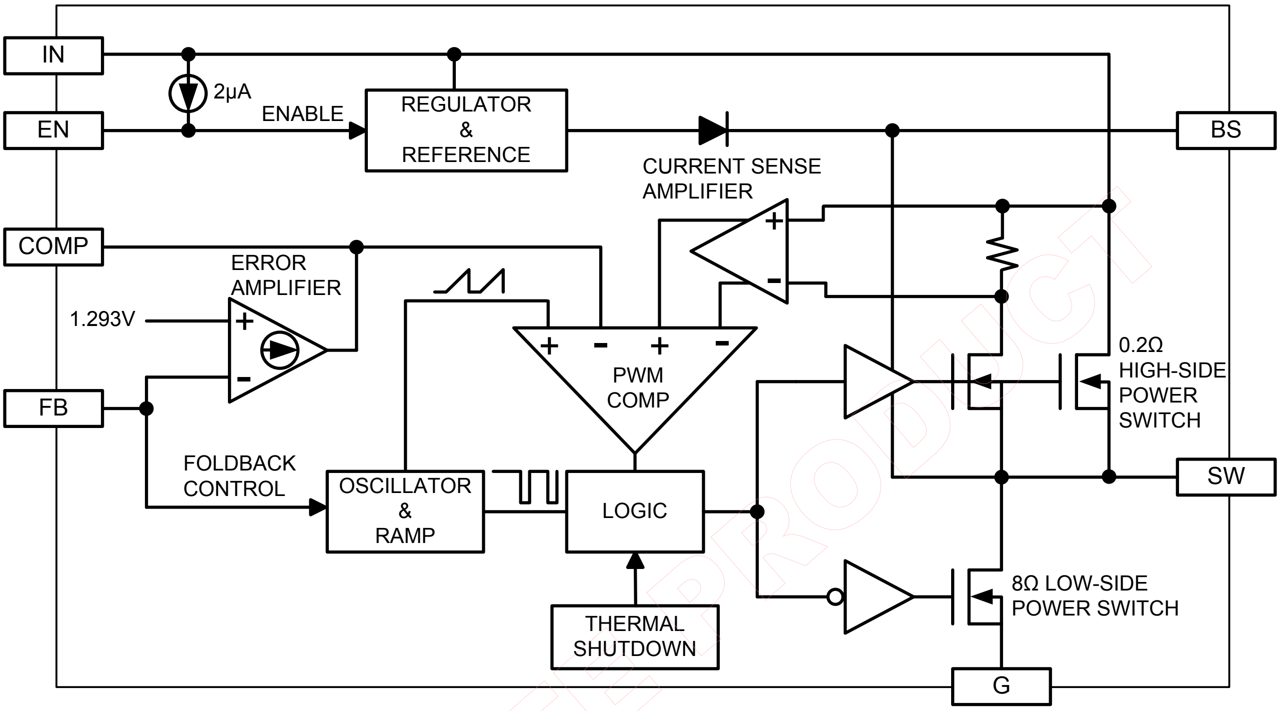
①: Do not exceed these limits to prevent damage to the device. Exposure to absolute maximum rating conditions for long periods may affect device reliability.

ELECTRICAL CHARACTERISTICS

(V_{IN} = 12V, T_J = 25°C, unless otherwise specified.)

PARAMETER	SYMBOL	TEST CONDITIONS	MIN	TYP	MAX	UNIT
Input Voltage	V_{IN}	V_{OUT} = 5V, I_{LOAD} = 1A	6		28	V
Feedback Voltage	V_{FB}	V_{COMP} = 1.5V	1.267	1.293	1.319	V
High-Side Switch On Resistance	R_{ONH}			0.2		Ω
Low-Side Switch On Resistance	R_{ONL}			8		Ω
SW Leakage		V_{EN} = 0		0	10	µA
Current Limit	I_{LIM}		3	3.5		A
COMP to Current Limit Transconductance	G_{COMP}			1.8		A/V
Error Amplifier Transconductance	G_{EA}	ΔI_{COMP} = ±10µA		550		µA/V
Error Amplifier DC Gain	A_{VEA}			4000		V/V
Switching Frequency	f_{SW}		160	200	240	kHz
Short Circuit Switching Frequency		V_{FB} = 0		50		kHz
Maximum Duty Cycle	D_{MAX}	V_{FB} = 1.1V		93		%
Minimum Duty Cycle		V_{FB} = 1.4V			0	%
Enable Threshold Voltage		Hysteresis = 0.1V	0.7	1	1.3	V
Enable Pull-Up Current		Pin pulled up to 4.5V typically when left unconnected		2		µA
Supply Current in Shutdown		V_{EN} = 0		8	20	µA
IC Supply Current in Operation		V_{EN} = 3V, V_{FB} = 1.4V		0.7		mA
Thermal Shutdown Temperature		Hysteresis = 10°C		160		°C

FUNCTIONAL BLOCK DIAGRAM



FUNCTIONAL DESCRIPTION

As seen in, *Functional Block Diagram*, the ACT4065 is a current mode pulse width modulation (PWM) converter. The converter operates as follows:

A switching cycle starts when the rising edge of the Oscillator clock output causes the High-Side Power Switch to turn on and the Low-Side Power Switch to turn off. With the SW side of the inductor now connected to IN, the inductor current ramps up to store energy in its magnetic field. The inductor current level is measured by the Current Sense Amplifier and added to the Oscillator ramp signal. If the resulting summation is higher than the COMP voltage, the output of the PWM Comparator goes high. When this happens or when Oscillator clock output goes low, the High-Side Power Switch turns off and the Low-Side Power Switch turns on. At this point, the SW side of the inductor swings to a diode voltage below ground, causing the inductor current to decrease and magnetic energy to be transferred to the output. This state continues until the cycle starts again.

The High-Side Power Switch is driven by logic using the BS bootstrap pin as the positive rail. This pin is charged to V_{SW} + 6V when the Low-Side Power Switch turns on.

The COMP voltage is the integration of the error between the FB input and the internal 1.293V reference. If FB is lower than the reference voltage, COMP tends to go higher to increase current to the output. Current limit happens when COMP reaches its maximum clamp value of 2.55V.

The Oscillator normally switches at 200kHz. However, if the FB voltage is less than 0.7V, then the switching frequency decreases until it reaches a minimum of 50kHz at V_{FB} = 0.5V.

Shutdown Control

The ACT4065 has an enable input EN for turning the IC on or off. When EN is less than 0.7V, the IC is in 8μA low current shutdown mode . When EN is higher than 1.3V, the IC is in normal operation mode. EN is internally pulled up with a 2μA current source and can be left unconnected for always-on operation. Note that EN is a low voltage of 6V; it should never be directly connected to IN.

Thermal Shutdown

The ACT4065 automatically turns off when its junction temperature exceeds 160°C.

APPLICATIONS INFORMATION

Output Voltage Setting

Figure 1:

Output Voltage Setting

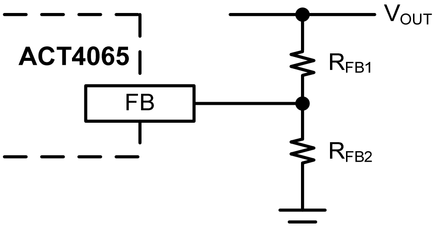


Figure 1 shows the connections for setting the output voltage. Select the proper ratio of the two feedback resistors R_{FB1} and R_{FB2} based on the output voltage. Typically, use $R_{FB2} \approx 10k\Omega$ and determine R_{FB1} from the output voltage:

$$R_{FB1} = R_{FB2}\left(\frac{V_{OUT}}{1.293V} - 1\right) \qquad (1)$$

Inductor Selection

The inductor maintains a continuous current to the output load. This inductor current has a ripple that is dependent on the inductance value: higher inductance reduces the peak-to-peak ripple current. The trade off for high inductance value is the increase in inductor core size and series resistance, and the reduction in current handling capability. In general, select an inductance value L based on ripple current requirement:

$$L = \frac{V_{OUT} \times (V_{IN} - V_{OUT})}{V_{IN} f_{SW} I_{OUTMAX} K_{RIPPLE}} \qquad (2)$$

where V_{IN} is the input voltage, V_{OUT} is the output voltage, f_{SW} is the switching frequency, I_{OUTMAX} is the maximum output current, and K_{RIPPLE} is the ripple factor. Typically, choose K_{RIPPLE} = 30% to correspond to the peak-to-peak ripple current being 30% of the maximum output current.

With this inductor value (Table 1), the peak inductor current is $I_{OUT} \times (1 + K_{RIPPLE} / 2)$. Make sure that this peak inductor current is less that the 3A current limit. Finally, select the inductor core size so that it does not saturate at 3A.

Table 1.

Typical Inductor Values

V_{OUT}	1.5V	1.8V	2.5V	3.3V	5V
L	10µH	10µH	15µH	22µH	33µH

Input Capacitor

The input capacitor needs to be carefully selected to maintain sufficiently low ripple at the supply input of the converter. A low ESR capacitor is highly recommended. Since a large current flows in and out of this capacitor during switching, its ESR also affects efficiency.

The input capacitance needs to be higher than 10µF. The best choice is the ceramic type; however, low ESR tantalum or electrolytic types may also be used provided that the RMS ripple current rating is higher than 50% of the output current. The input capacitor should be placed close to the IN and G pins of the IC, with shortest possible traces. In the case of tantalum or electrolytic types, they can be further away if a small parallel 0.1µF ceramic capacitor is placed right next to the IC.

Output Capacitor

The output capacitor also needs to have low ESR to keep low output voltage ripple. The output ripple voltage is:

$$V_{RIPPLE} = I_{OUTMAX} K_{RIPPLE} R_{ESR} + \left(\frac{V_{IN}}{28 \times f_{SW}^{2} L C_{OUT}}\right) \qquad (3)$$

where I_{OUTMAX} is the maximum output current, K_{RIPPLE} is the ripple factor, R_{ESR} is the ESR resistance of the output capacitor, f_{SW} is the switching frequency, L is the inductor value, C_{OUT} is the output capacitance, R_{ESR} is very small and does not contribute to the ripple. Therefore, a lower capacitance value can be used for ceramic type. In the case of tantalum or electrolytic type, the ripple is dominated by R_{ESR} multiplied by the ripple current. In that case, the output capacitor is chosen to have sufficiently low ESR.

For ceramic output type, typically choose a capacitance of about 22µF. For tantalum or electrolytic type, choose a capacitor with less than 50mΩ ESR.

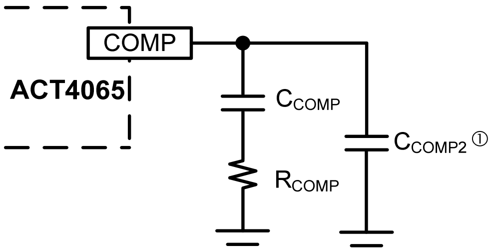
Rectifier Diode

Use a Schotky diode as the rectifier to conduct current when the High-Side Power Switch is off. The Schottky diode must have current rating higher than the maximum output current and the reverse voltage rating higher than the maximum input voltage.

Stability compensation

Figure 2:

Stability Compensation



①: C_{COMP2} is needed only for high ESR output capacitors

The feedback system of the IC is stabilized by the components at COMP pin, as shown in Figure 2. The DC loop gain of the system is determined by the following equation:

$$A_{VDC} = \frac{1.293V}{I_{OUT}} A_{VEA} G_{COMP} \qquad (4)$$

The dominant pole P1 is due to C_{COMP}:

$$f_{P1} = \frac{G_{EA}}{2\pi A_{VEA} C_{COMP}} \qquad (5)$$

The second pole P2 is the output pole:

$$f_{P2} = \frac{I_{OUT}}{2\pi V_{OUT} C_{OUT}} \qquad (6)$$

The first zero Z1 is due to R_{COMP} and C_{COMP}:

$$f_{Z1} = \frac{1}{2\pi R_{COMP} C_{COMP}} \qquad (7)$$

And finally, the third pole is due to R_{COMP} and C_{COMP2} (if C_{COMP2} is used):

$$f_{P3} = \frac{1}{2\pi R_{COMP} C_{COMP2}} \qquad (8)$$

Follow the following steps to compensate the IC:

STEP 1. Set the cross over frequency at 1/5 of the switching frequency via R_{COMP}:

$$R_{COMP} = \frac{2\pi V_{OUT} C_{OUT} f_{SW}}{10 G_{EA} G_{COMP} \times 1.293V}$$

$$= 9.8 \times 10^{7} V_{OUT} C_{OUT} \quad (\Omega) \qquad (9)$$

but limit R_{COMP} to 15kΩ maximum.

STEP 2. Set the zero f_{Z1} at 1/4 of the cross over frequency. If R_{COMP} is less than 15kΩ, the equation for C_{COMP} is:

$$C_{COMP} = \frac{1.6 \times 10^{-5}}{R_{COMP}} \quad (F) \qquad (10)$$

If R_{COMP} is limited to 15kΩ, then the actual cross over frequency is 6.1/ ($V_{OUT}C_{OUT}$). Therefore:

$$C_{COMP} = 6.96 \times 10^{-6} V_{OUT} C_{OUT} \quad (F) \qquad (11)$$

STEP 3. If the output capacitors ESR is high enough to cause a zero at lower than 4 times the cross over frequency, an additional compensation capacitor C_{COMP2} is required. The condition for using C_{COMP2} is required. The condition for using C_{COMP2} is:

$$R_{ESROUT} \geq Min\left(\frac{1.1 \times 10^{-6}}{C_{OUT}}, 0.012V_{OUT}\right) \quad (\Omega) \qquad (12)$$

And the proper value for C_{COMP2} is:

$$C_{COMP2} = \frac{C_{OUT} R_{ESROUT}}{R_{COMP}} \qquad (13)$$

Though C_{COMP2} is unnecessary when the output capacitor has sufficiently low ESR, a small value C_{COMP2} such as 100pF may improve stability against PCB layout parasitic effects.

Table 2 shows some calculated results based on the compensation method above.

Table 2:

Typical Compensation for Different Output voltages and Output Capacitors

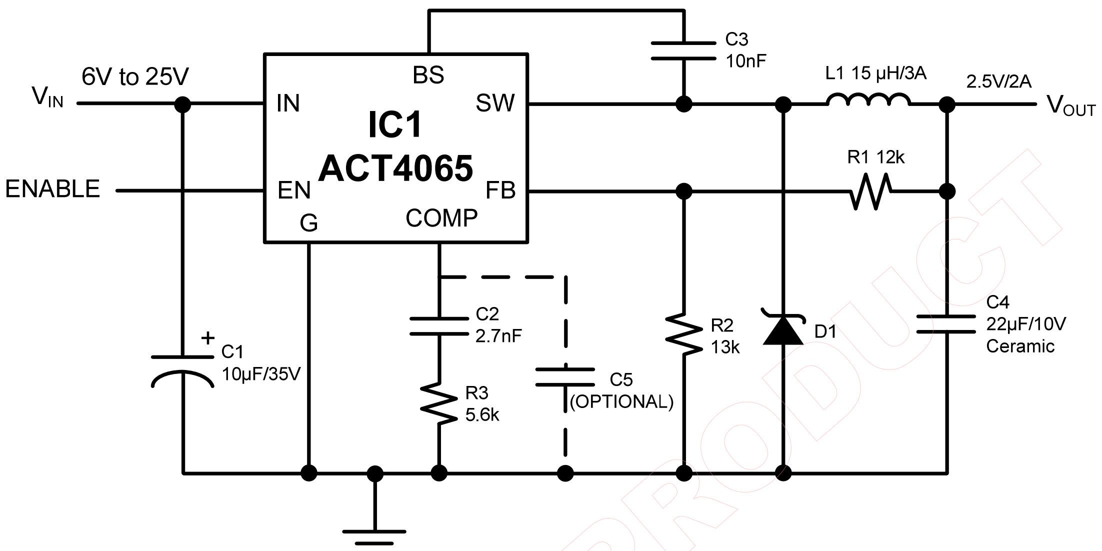
V_{OUT}	C_{OUT}	R_{COMP}	C_{COMP}	C_{COMP2} ①
2.5V	22µF Ceramic	5.6kΩ	2.7nF	None
3.3V	22µF Ceramic	7.2kΩ	2.2nF	None
5V	22µF Ceramic	10kΩ	2.2nF	None
2.5V	47µF SP Cap	11kΩ	1.5nF	None
3.3V	47µF SP Cap	15kΩ	1nF	None
5V	47µF SP Cap	15kΩ	1.5nF	None
2.5V	470µF/6.3V/30mΩ	15kΩ	8.2nF	1nF
3.3V	470µF/6.3V/30mΩ	15kΩ	10nF	1nF
5V	470µF/10V/30mΩ	15kΩ	15nF	None

①: C_{COMP2} is needed only for high ESR output capacitors

Figure 3 shows a sample ACT4065 application circuit generating a 2.5V/2A output.

Figure 3:

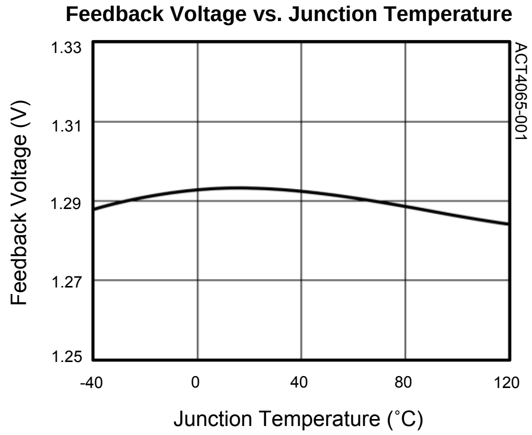
ACT4065 2.5V/2A Output Application①

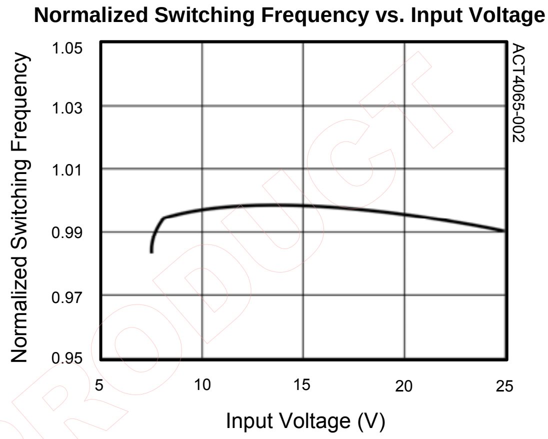


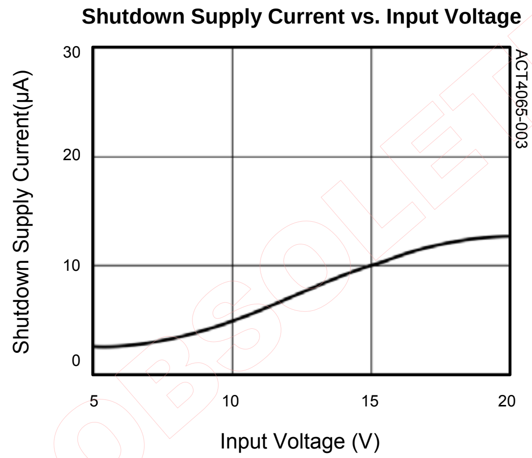
①: D1 is a 40V, 3A Schottky diode with low forward voltage, an IR 30BQ040 or SK34 equivalent. C4 can be either a ceramic capacitor (Panasonic ECJ-3YB1C226M) or SP-CAP (Specialty Polymer) Aluminum Electrolytic Capacitor such as Panasonic EEFCD0J470XR. The SP-Cap is based on aluminum electrolytic capacitor technology, but uses a solid polymer electrolyte and has very stable capacitance characteristics in both operating temperature and frequency compared to ceramic, polymer, and low ESR tantalum capacitors.

TYPICAL PERFORMANCE CHARACTERISTICS

(Circuit of Figure 3, unless otherwise specified .)

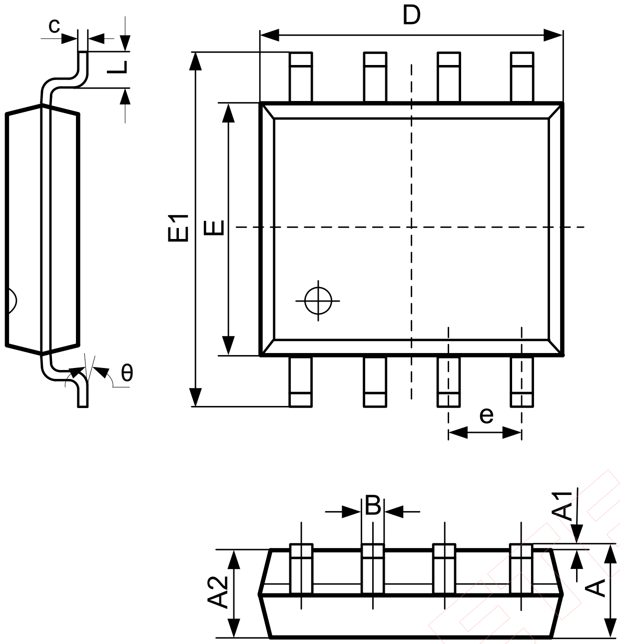






PACKAGE OUTLINE

SOP-8 PACKAGE OUTLINE AND DIMENSIONS



SYMBOL	DIMENSION IN MILLIMETERS		DIMENSION IN INCHES	
	MIN	MAX	MIN	MAX
A	1.350	1.750	0.053	0.069
A1	0.100	0.250	0.004	0.010
A2	1.350	1.550	0.053	0.061
B	0.330	0.510	0.013	0.020
C	0.190	0.250	0.007	0.010
D	4.780	5.000	0.188	0.197
E	3.800	4.000	0.150	0.157
E1	5.800	6.300	0.228	0.248
e	1.270 TYP		0.050 TYP	
L	0.400	1.270	0.016	0.050
θ	0°	8°	0°	8°